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2. Patent application number *(The Patent Office will fill in this part)*	0322538.0
3. Full name, address and postcode of the or of each applicant *(underline all surnames)*	The Queen's University of Belfast University Road Belfast BT7 1NN United Kingdom
Patents ADP number *(if you know it)*	772798001
If the applicant is a corporate body, give the country/state of its incorporation	United Kingdom
4. Title of the invention	"Phase Conjugate Circuit"
5. Name of your agent *(if you have one)*	Murgitroyd & Company
"Address for service" in the United Kingdom to which all correspondence should be sent *(including the postcode)*	Scotland House 165-169 Scotland Street Glasgow G5 8PL
Patents ADP number *(if you know it)*	1198015

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Murgitroyd & Company

12. Name and daytime telephone number of person to contact in the United Kingdom   KEITH JONES   0141 307 8400

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Phase Conjugate Circuit

This invention relates generally to phase conjugate circuits and specifically, but not exclusively, to phase conjugate circuits containing phase locked loop circuits.

Phase conjugation of a particular signal is useful in numerous applications. One example is in retro-directive antenna arrays, where an incoming signal is automatically re-transmitted in the same direction as it was incident on the array by transmitting the phase conjugate of the incoming signal. Another example is in LINC (Linear Amplification using Non-Linear Components) amplifiers, where an amplitude modulated signal is firstly converted to a phase modulated signal and a phase conjugate modulated signal before being

amplified by non-linear amplifiers. The two amplified signals are then recombined to provide an amplified version of the original signal.

In both these applications obtaining the phase conjugate of the incoming signal is an essential part of the electrical circuit.

Phase conjugation circuitry, to some extent, has limited the commercialisation of both Retro-directive antenna arrays and LINC circuit architectures. For example, prior art phase conjugate circuits for retro-directive arrays use a heterodyning approach involving a signal mixer which relies on a local oscillator (LO) operating at twice the desired input RF (Radio Frequency) frequency. As the RF signal and the signal from the output IF (Intermediate Frequency) ports are the same, or very nearly the same, direct leakage from the RF signal to the IF ports causes significant problems. In addition the LO frequency must be twice the RF frequency so that the down-converted IF output signal is the phase conjugate of the RF input signal. This can be disadvantageous when the RF signal is required to be of very high frequency such as for anti-collision vehicular radars operating at 77 GHz. In this case, the LO frequency would have to be 154GHz which would be difficult to construct using currently available technology.

LINC amplifiers suffer from general circuit complexity in the phase conjugate sections.

Subsequently, LINC amplifiers have not been successfully operated at frequencies of greater than a few 10's of Megahertz mainly for this reason.

Additional problems exist with the prior art associated with phase conjugation circuitry prominent amongst these are the requirement for:

- sophisticated mixer balancing techniques required to prevent unwanted leakage signals corrupting the phase conjugation process. This leads to weak output signal levels since conventional mixer circuits are either passive (and therefore lossy) or limited to the few dB conversion gain that can be achieved with conventional active mixers; and
- the need for a local oscillator signal operating at twice the RF signal (as mentioned above).

Other applications for retrodirective (self tracking) array technology include simplex and duplex communication with low earth orbiting, non-geosynchronous satellites and as a low cost means for automatic beamforming as required for modern spatial division multiple access mobile phone wireless communication systems. Further examples are the use of a self-tracking array for automatic alignment of ground stations with high altitude communications platforms or in the creation of agile radar crossection modification.

Phase locked loop circuits have been widely used since first being proposed in 1922. Since that time,

PLL's have been used in instrumentation, space telemetry and many other applications requiring a high degree of noise immunity and narrow bandwidth.

A standard phase lock loop circuit comprises a phase detector, a low-pass filter, and an oscillator, usually a voltage-controlled oscillator (VCO). In the case where the oscillator is a VCO, the phase detector outputs a voltage proportional to the phase difference between a PLL input and a feedback signal from the output of the VCO. The low-pass filter acts as an integrator and provides a filtered voltage signal or an error signal which controls the VCO. When the error signal is zero, the VCO operates at a set frequency, known as the free running frequency. When the error signal is not zero, the phase of the PLL input and the feedback signal are no longer in balance and the VCO reacts to the error signal by modifying its output to track the PLL input.

It as an object of the present invention to obviate or mitigate the problems identified above in relation to phase conjugation circuits.

According to a first aspect of the present invention there is provided a method of deriving phase conjugation information from an input signal of a given first frequency, the method comprising mixing the input signal with the output of an oscillator forming part of a phase locked loop (PLL) circuit having a reference input signal of a second

frequency which is proportional to the first frequency.

According to a second aspect of the present invention there is provided a circuit arrangement for deriving phase conjugation information from a main input signal of a given frequency comprising:

at least one phase locked loop circuit comprising a reference input signal, a feedback signal, at least one phase detecting means and an oscillator having a main output signal;

at least one heterodyne mixer;

wherein the phase detection means detects any phase difference between the reference input signal and the feedback signal and provides a phase control signal to the oscillator, and the heterodyne mixer mixes the main input signal and the main output signal to provide the feedback signal.

Preferably the oscillator is a voltage controlled oscillator (VCO).

Preferably the feedback signal is the up-converted mixing product of the heterodyne mixer.

Preferably, the frequency of the reference input signal is scaled to match the frequency of the feedback signal.

Further preferably, the feedback signal is scaled.

Preferably, the phase detection means is a digital phase detector.

In one form of the invention, the phase detection means also detects any phase difference between the main output signal and the reference signal thereby creating a further phase locked loop.

Preferably, the phase detection means comprises:

a first phase detector which detects any phase difference between the reference input signal and the feedback signal;

a second phase detector which detects any phase difference between the reference input signal and the main output signal;

an integrator integrating the first phase detector output;

a heterodyne mixer mixing the integrator output and the second phase detector output;

wherein the mixer output is the phase detection means output providing a control signal for the oscillator.

In an alternative form of the invention, the phase detection means comprises:

a first phase detection heterodyne mixer mixing the reference input signal and the feedback signal and having a first phase detection mixer output wherein the first mixer output is the down-converted mixing product of the first mixer;

a second phase detection heterodyne mixer mixing the reference input signal and the first

phase detection mixer output and having a second phase detection mixer output wherein the second phase detection mixer output is the down-converted mixing product of the second phase detection mixer and the phase detection means output providing a control signal for the oscillator.

Embodiments of the present invention will now be described with reference to the accompanying drawings, in which;

Fig. 1 shows a schematic diagram of a frequency offset phase conjugating phase locked loop (PLL) circuit;

Fig. 2 shows a schematic diagram of a practical implementation of the phase conjugating PLL circuit of Fig. 1;

Fig. 3 shows a graphical representation of experimentally derived phase angle of signals in the phase conjugating PLL circuit of Fig. 2;

Fig. 4 shows a schematic diagram of an integrator based phase conjugating PLL circuit;

Fig. 5 shows a schematic diagram of a heterodyne mixer based phase conjugating PLL circuit.

Referring now to Fig. 1, a frequency offset phase conjugating PLL circuit 100 has a main input signal 102 ($F_{in}+\phi$) and a reference input signal 104 (F_{REF}). A

reference divider 106 divides the reference input signal 104 and a main divider 108 divides a feedback signal 109 such that a phase detector 110 receives the divided reference input signal and the divided feedback signal at the same frequency. The phase detector outputs a phase control signal representing a phase difference between the reference input signal and the feedback signal 109. A low-pass loop filter 112 filters, or integrates, the phase control signal to provide a DC control signal. A voltage controlled oscillator (VCO) 114 receives the phase control signal and outputs a VCO signal 116 of a particular frequency (F_{VCO}) and a phase angle (φ) determined by the phase control signal. The VCO signal 116 is also a phase conjugate signal of the main input signal 102 as explained below. A heterodyne mixer 118 mixes the VCO signal 116 and the main input signal 102 to produce the feedback signal 109 which in this case is filtered by a band pass filter 120 to allow selection of the up-converted mixing product of the mixer 118.

The frequency offset phase conjugating PLL circuit 100 works in the following manner:

Up-converted Phase locked Loop without reference divider 106 and main divider 108

Output of mixer 118 : $F_{IN}+\phi + F_{VCO}+\varphi$

Reference Input 104 : $F_{REF} = F_{IN} + F_{VCO}$

At position C : $F_{IN} + F_{VCO} = F_{IN}+\phi + F_{VCO}+\varphi$

: $F_{IN} + F_{VCO} - F_{IN}-\phi + F_{VCO}-\varphi = 0$

$$: -\phi - \varphi = 0$$

$$: \varphi = -\phi$$

VCO signal 116 $: F_{VCO} + \varphi = F_{VCO} - \phi$

Therefore, if $F_{VCO} = F_{IN}$, the VCO signal 116 is the phase conjugate of the main input signal 102. If $F_{VCO} \neq F_{IN}$ then the VCO signal 116 is the offset phase conjugate of the main input signal 102.

The reference divider 106 and the main divider 108 allow the possibility of reducing the required frequency of the reference input signal 104. The phase detector 110 is intended to detect any difference in phase between the feedback signal 109 and the reference input signal 104.

For example:

F_{IN} = 1000Mhz
F_{VCO} = 990Mhz
F_{REF} = 10Mhz
Input to Main divider (up-converted) = 1990Mhz
Output from Main divider = 1990/9950 = 0.2MHz
Input to Reference divider = 10Mhz
Output from Reference divider = 10/50 = 0.2MHz

Using this arrangement, the reference input signal 104 at a much smaller frequency than the main input signal 102 is required.

Referring now to Fig. 2, a phase conjugating PLL circuit 200, that is an experimental implementation of the frequency offset phase conjugating PLL

circuit of Fig. 1, is shown. A main input signal 202 and a reference input signal 204 are generated from a first signal synthesiser 206. A phase shifter 203 is introduced to the main input signal 202 so that the main input signal 202 has a different phase angle than that of the reference input signal 204. A first power splitter 205 splits the main input signal 202 so that an oscilloscope 230 can visually display the signal 202 without any losses. A Philips® UMA1021M PLL chip contains a reference input divider 210, a main input divider 212 and a phase detector 214. In this example, the reference input divider 210 divides the reference input signal 204 which is then inputted to the phase detector 214. The main input divider 212 divides a feedback signal 216 which is then also inputted to the phase detector 214. The phase detector produces a phase control signal 218 which represents the phase difference between the reference input signal 204 and the feedback signal 216. A loop filter 220 integrates the phase control signal 218. A unity gain non-inverting summing amplifier 222 ensures the phase control signal 218 is isolated from the phase detector 214 and also allows the phase control signal 218 to be offset as necessary. A Voltage Controlled Oscillator (VCO) 224 has an output signal 226 at a predetermined frequency. The VCO can vary the phase of the output signal 226 dependent on the phase control signal 218. A second power splitter 228 allows the output signal 226 to be displayed on the oscilloscope 230 without any losses within the circuit 200. The output signal 226, when the circuit

200 is phase locked, is now a phase conjugate signal of the main input signal 202. A heterodyne mixer 232 mixes the output signal 226 and the main input signal 202 to produce the feedback signal 216. A band-pass filter 234 filters the feedback signal 216 such that only the up-converted mixing product from the mixer 232 remains. A third power splitter 236 allows the feedback signal to be analysed by a microwave transition analyser (MTA) 238 as well as being connected to the main divider 212 without any losses to the circuit 200. A second signal synthesiser 240 provides a comparison signal 242 to the oscilloscope 230 and the MTA 238 as required. The main input signal 202 and the comparison signal 242 are phase locked to the reference input signal.

In use, the first signal synthesiser 206 synthesised the main input signal 202 at a frequency of 1.05GHz and the reference input signal 204 at 0.01GHz. The phase shifter 203 introduces a different phase angle to the main input signal 202 than that of the reference input signal 204. The main input signal 202 is then viewed on the oscilloscope 230 via the first power splitter 205. The main output signal 226 is generated by the VCO 224 at a frequency of 0.94GHz and is also viewed on the oscilloscope 230 via the second power splitter 228. The mixer 232 mixes the main input signal 202 and the main output signal 226. The band-pass filter 234 ensures that only the up-converted mixing product forms the feedback signal 216 at a frequency of 1.99Ghz. The feedback signal 216 is viewed on the MTA 238 via the

third power splitter 236. The main input divider 212 divides the feedback signal 216 by 9950 producing a signal of 200KHz. The reference divider divide the reference input signal 204 by 50 to also produce a signal of 200KHz. The phase detector 214 then detects the phase difference between the divided feedback signal 216 and the divided reference input signal 204 to produce the phase control signal 218 which ultimately controls the VCO's 224 phase angle. The second signal synthesiser 240 is used to generate different signals as required for comparison purposes. Therefore, the comparison signal 242 is set to 0.94GHz for comparison with the main output signal. As the comparison signal 242 is phase locked to the reference input signal 202, the main output signal 226 should be a phase conjugate of the comparison signal and therefore the phase difference can be measured to confirm this. To measure the actual phase of the main input signal 202 after it had been phase shifted by the phase shifter 203, the second synthesised source 240 is set to produce a comparison signal 242 of 1.05GHz. To further validate that phase conjugation was operating correctly it was important that the feedback signal 216 had constant phase. The second synthesised source 240 is set to produce a comparison signal 242 of 1.99GHz and the MTA 238 used to analyse the feedback signal 216.

Referring now to Fig. 3 a graphical representation of a non-conjugated phase angle 302 (representing the main input signal 202 of Fig.2) is matched

substantially equally and oppositely to a conjugated angle 304 (representing the output signal 226 of Fig. 2). A conjugation error 306 is also shown representing the error in phase angle in the conjugated angle 304. It can be clearly seen from Fig. 3 that the conjugated angle 304 has only a small conjugation error 306 at any time and that the practical implementation circuit 202 effectively produces a frequency offset phase conjugated output.

Referring now to Fig. 4, an alternative embodiment of a phase conjugation PLL circuit 400 is shown. The circuit 400 has a PLL 402 and a loop 404. A reference signal 406 supplies a reference signal to both the PLL 402 and the loop 404. The PLL 402 has a first phase detector 408 which compares a first feedback signal 410 with the reference signal 406. A summer 412 receives a first phase error signal 414 and a second phase error signal 416 to produce a composite phase control signal 418. A VCO 419 produces an output signal 420 with a phase dependent on the phase control signal 418. A second heterodyne mixer 422 mixes a main input signal 424 with the output signal 420 to produce a second feedback signal 426. A second phase detector 428 compares the phase of the second feedback signal and the reference signal 406 producing a second phase detector output 430. An integrator 432 integrates the second phase detector output 430 producing the second phase error signal 416.

In use, the circuit 400 has a fast acting PLL 402 that establishes a frequency lock. The loop 404 is relatively slower because of the integrator's 432 transfer characteristics. The loop 404 then forces the output signal 420 to the conjugate phase of the main input signal 424.

Referring now to Fig. 5, an alternative embodiment of a phase conjugation PLL circuit 500 is shown. A first heterodyne mixer 502 mixes a main input signal 504 and an output signal 506 to produce a feedback signal 508. The feedback signal 508 is the up-converted mixing product of the first heterodyne mixer 502. A second heterodyne mixer 510 mixes a reference signal 512 with the feedback signal 508 producing an intermediate signal 514. The intermediate signal 514 is the down-converted mixing product of the second heterodyne mixer 510. A third heterodyne mixer 516 mixes the intermediate signal 514 with the reference signal 512 producing a phase control signal 518. The phase control signal 518 is the down-converted mixing product of the third heterodyne mixer 516. A VCO 520 produces an output signal 506 with a phase dependent on the phase control signal 518.

The operation of the circuit 500 is explained below.

Assuming that the circuit 500 is phase locked and the main input signal (RF_{IN}) 504, the output signal (RF_{OUT}) 506 and the reference signal (RF_{REF}) 512 are all the same frequency ω.

The feedback signal 508 is RF_F, the intermediate signal 514 is RF_I and the phase control signal 518 is RF_C.

$$RF_{REF} = \omega + \theta_{REF}$$
$$RF_{IN} = \omega + \theta_{IN}$$
$$RF_{OUT} = \omega + \theta_{OUT}$$
$$RF_F = 2\omega + \theta_{OUT} + \theta_{IN}$$
$$RF_I = \omega + \theta_{OUT} + \theta_{IN} - \theta_{REF}$$
$$RF_C = \theta_{OUT} + \theta_{IN} - \theta_{REF} - \theta_{REF} = c$$
$$\theta_{OUT} = c + 2\theta_{REF} - \theta_{IN}$$

In the equation above it is shown that the output signal phase is conjugated to the main input signal phase ($\theta_{OUT} = -\theta_{IN}$). The term $c + 2\theta_{REF}$ represents a static phase error introduced by the reference input signal's 512 oscillator. The $2\theta_{REF}$ term may be trimmed removed by filtering. The term c represents the control voltage for the VCO 520 and therefore will always be present except where the output frequency is equal to the free-running frequency of the VCO 520. The term c will change as the circuit 500 tracks changes in the main input signal 504 frequency.

For retrodirective antenna arrays this does not pose a problem as relative phase states are important, not absolute phase states. For LINC type amplifier applications any phase error caused by the term c can be accounted for by a prior calibration process

across the expected frequency operating range of the circuit.

The circuit 500 can instantaneously phase conjugate as the circuit is made up of heterodyne mixers and does not include integrators or phase detectors which have a finite time determined by the loop dynamics in order to establish a phase lock. As the heterodyne mixers act as the phase detectors, the circuit 500 can operate directly at the microwave and millimetre wave frequencies without the need for dividers or digital phase detection circuitry.

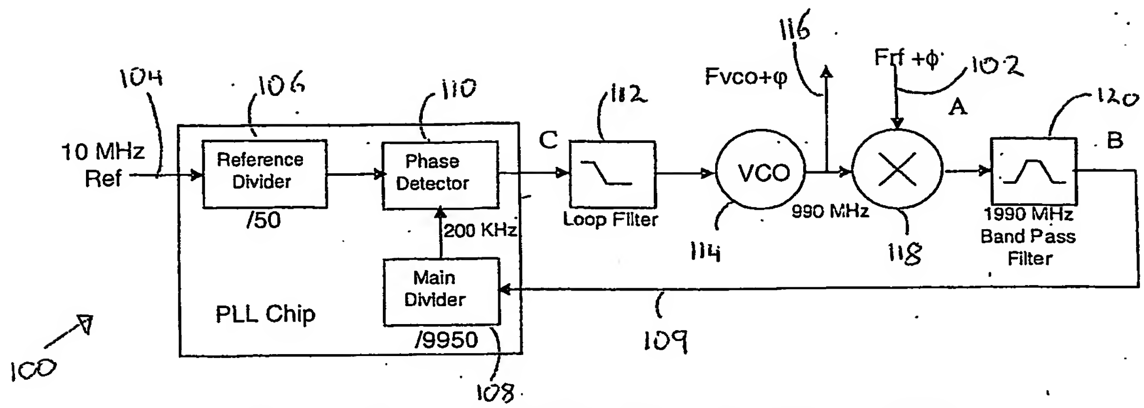

Figure 1 Frequency Offset Phase Conjugating PLL

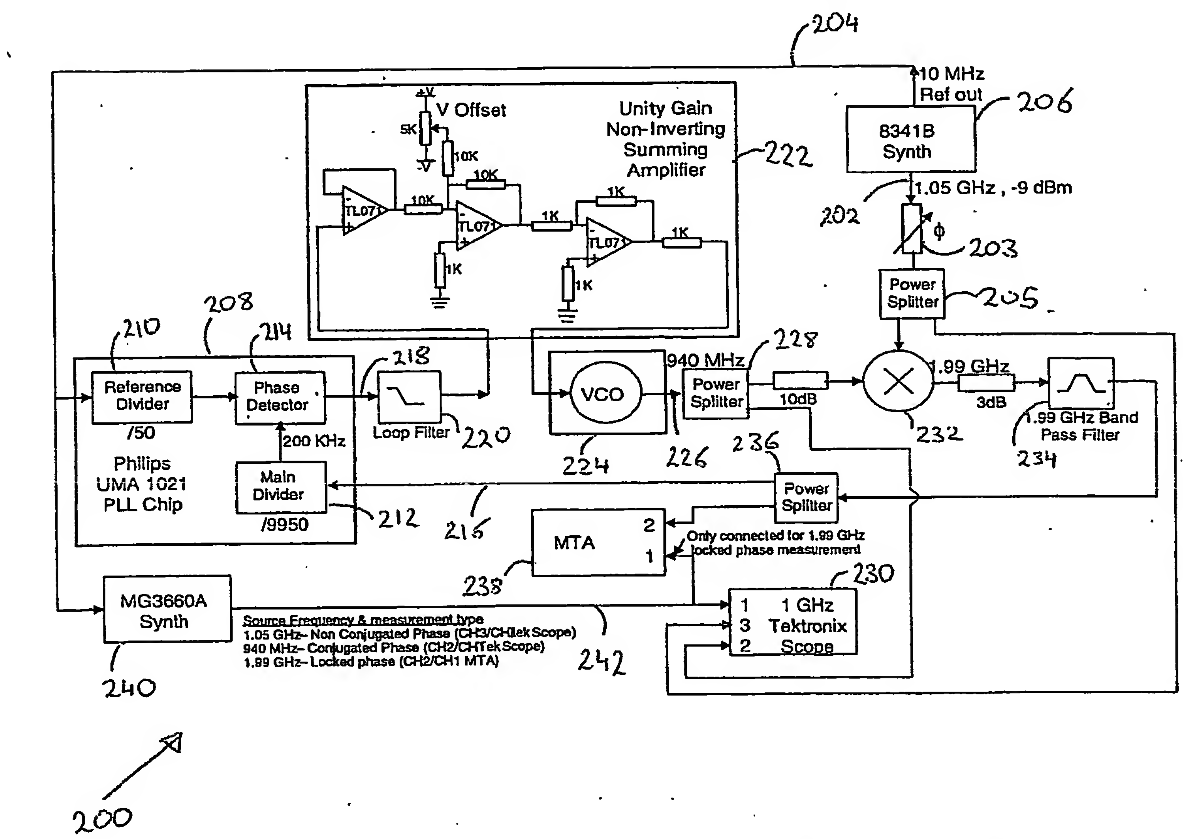

Figure 2 Experimental Set-up for Phase Conjugating PLL

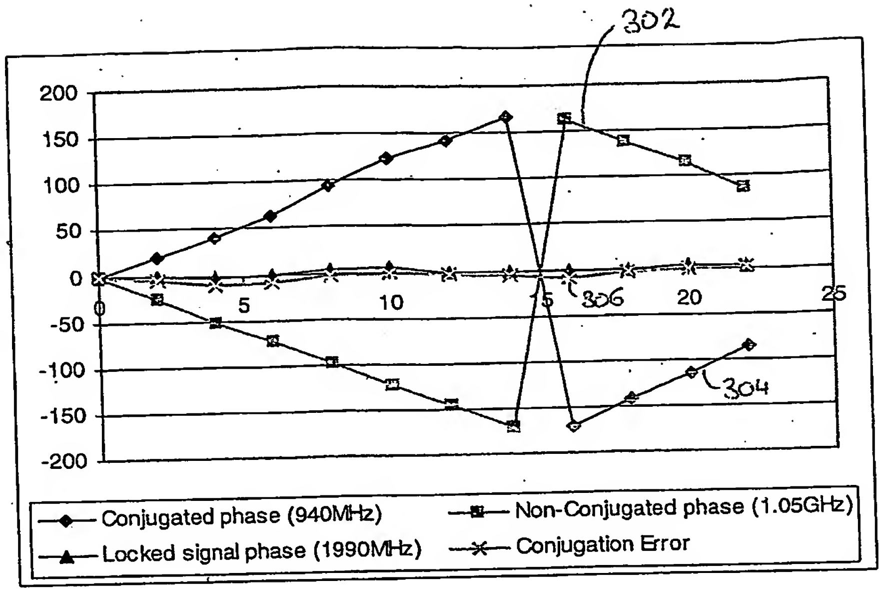

Figure 3 Frequency Offset Phase Conjugating Results

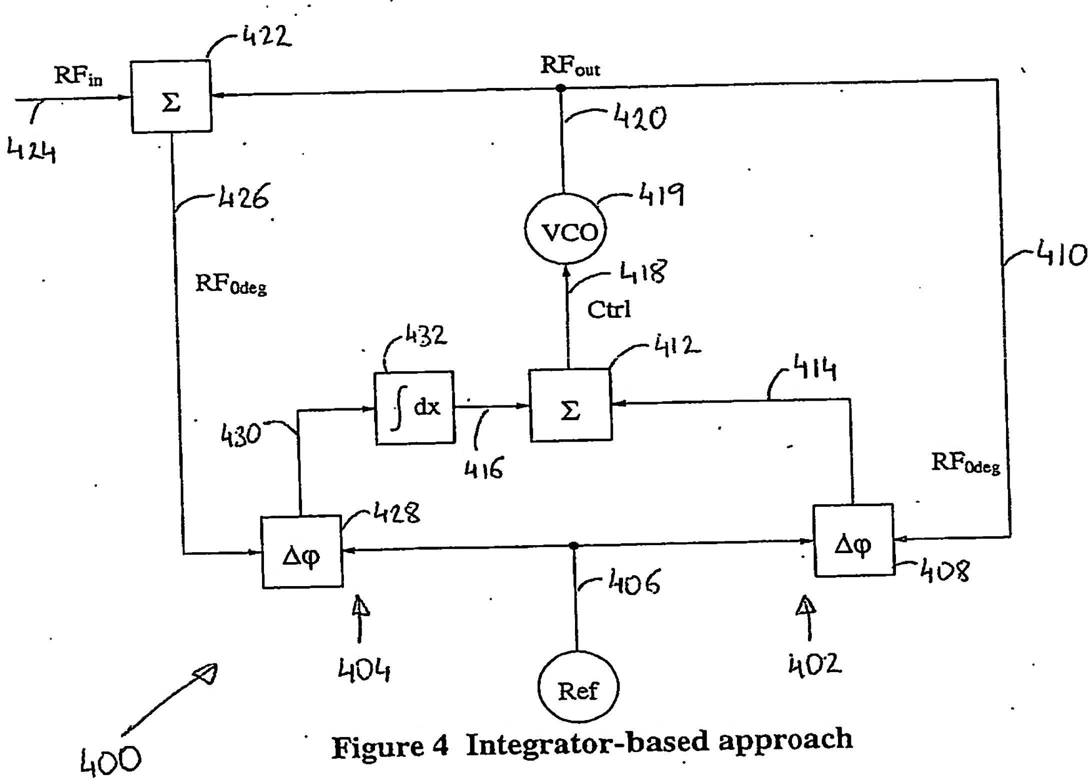

Figure 4 Integrator-based approach

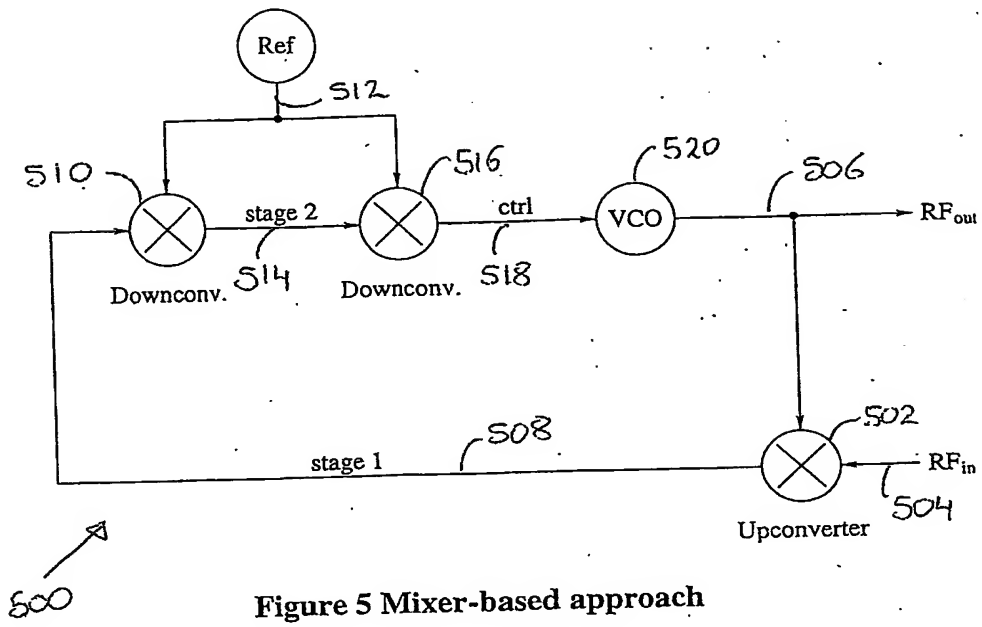

Figure 5 Mixer-based approach

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